

## FEATURES

- Ultralow noise: 2.8 nV/ $\sqrt{\text{Hz}}$  at 1 kHz typical**
- Ultralow distortion: 0.0002% typical**
- Low supply current: 1.8 mA per amplifier typical**
- Offset voltage: 1 mV maximum**
- Bandwidth: 6.5 MHz typical**
- Slew rate: 12 V/ $\mu\text{s}$  typical**
- Dual-supply operation:  $\pm 4.5\text{ V}$  to  $\pm 18\text{ V}$**
- Unity-gain stable**
- Extended industrial temperature range**
- 8-lead SOIC and 2 mm  $\times$  2 mm LFCSP packages**

## APPLICATIONS

- Precision instrumentation**
- Professional audio**
- Active filters**
- Low noise amplifier front end**
- Integrators**

## GENERAL DESCRIPTION

The ADA4075-2 is a dual, high performance, low noise operational amplifier combining excellent dc and ac characteristics on the Analog Devices, Inc., *iPolar*<sup>®</sup> process. The *iPolar* process is an advanced bipolar technology implementing vertical junction isolation with lateral trench isolation. This allows for low noise performance amplifiers in smaller die size at faster speed and lower power. Its high slew rate, low distortion, and ultralow noise make the ADA4075-2 ideal for high fidelity audio and high performance instrumentation applications. It is also especially useful for lower power demands, small enclosures, and high density applications. The ADA4075-2 is specified for the  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$  temperature range and is available in a standard SOIC package and a 2 mm  $\times$  2 mm LFCSP package.

## PIN CONFIGURATIONS

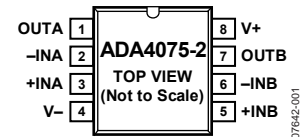


Figure 1. 8-Lead SOIC

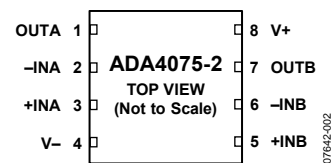


Figure 2. 8-Lead, 2 mm  $\times$  2 mm LFCSP

Table 1. Low Noise Precision Op Amps

Supply	44 V	36 V	12V to 16 V	5 V
Single	OP27	AD8671 AD8675 AD8597 ADA4004-1 AD797	AD8665 OP162	AD8605 AD8655 AD8691
Dual	OP275	AD8672 AD8676 AD8599 ADA4004-2	AD8666 OP262	AD8606 AD8656 AD8692
Quad		AD8674 ADA4004-4	AD8668 OP462	AD8608 AD8694

### Rev. B

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**REVISION HISTORY**

**12/11—Rev. A to Rev. B**

Changes to Features Section.....	1
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**8/09—Rev. 0 to Rev. A**

Added 8-Lead LFCSP_WD .....	Universal
Changes to Table 1 .....	1
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Changes to Table 4 and Table 5.....	5
Changes to Figure 3, Figure 5, Figure 6, and Figure 8 .....	6
Added Figure 4 and Figure 7; Renumbered Sequentially .....	6
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**10/08—Revision 0: Initial Version**

## SPECIFICATIONS

$V_{SY} = \pm 15\text{ V}$ ,  $V_{CM} = 0\text{ V}$ ,  $T_A = 25^\circ\text{C}$ , SOIC package, unless otherwise noted.

Table 2.

Parameter	Symbol	Conditions	Min	Typ	Max	Unit
<b>INPUT CHARACTERISTICS</b>						
Offset Voltage	$V_{OS}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		0.2	1	mV
Input Bias Current	$I_B$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		30	100	nA
Input Offset Current	$I_{OS}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		5	50	nA
Input Voltage Range		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	-12.5		+12.5	V
Common-Mode Rejection Ratio	CMRR	$V_{CM} = -12.5\text{ V to }+12.5\text{ V}$ $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	110	118		dB
Large Signal Voltage Gain	$A_{VO}$	$R_L = 2\text{ k}\Omega$ , $V_O = -11\text{ V to }+11\text{ V}$ $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	114	117		dB
		$R_L = 600\ \Omega$ , $V_O = -10\text{ V to }+10\text{ V}$ $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	112	117		dB
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	106			dB
Offset Voltage Drift	$\Delta V_{OS}/\Delta T$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		0.3		$\mu\text{V}/^\circ\text{C}$
Input Resistance, Differential Mode	$R_{INDM}$			1.5		M $\Omega$
Input Resistance, Common Mode	$R_{INCM}$			500		M $\Omega$
Input Capacitance, Differential Mode	$C_{INDM}$			2.4		pF
Input Capacitance, Common Mode	$C_{INCM}$			2.1		pF
<b>OUTPUT CHARACTERISTICS</b>						
Output Voltage High	$V_{OH}$	$R_L = 2\text{ k}\Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12.8	13		V
		$R_L = 600\ \Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12.5			V
		$V_{SY} = \pm 18\text{ V}$ , $R_L = 600\ \Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12.4	12.8		V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12			V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	15	15.8		V
Output Voltage Low	$V_{OL}$	$R_L = 2\text{ k}\Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		-14	-13.6	V
		$R_L = 600\ \Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			-13	V
		$V_{SY} = \pm 18\text{ V}$ , $R_L = 600\ \Omega$ to GND $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		-13.6	-13	V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			-12.5	V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		-16.6	-16	V
Short-Circuit Current	$I_{SC}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		40		mA
Closed-Loop Output Impedance	$Z_{OUT}$	$f = 1\text{ kHz}$ , $A_V = 1$		0.1		$\Omega$
<b>POWER SUPPLY</b>						
Power Supply Rejection Ratio	PSRR	$V_{SY} = \pm 4.5\text{ V to } \pm 18\text{ V}$ $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	106	110		dB
Supply Current per Amplifier	$I_{SY}$	$V_{SY} = \pm 4.5\text{ V to } \pm 18\text{ V}$ , $I_O = 0\text{ mA}$ $-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	100	1.8	2.25	mA
<b>DYNAMIC PERFORMANCE</b>						
Slew Rate	SR	$R_L = 2\text{ k}\Omega$ , $A_V = 1$		12		V/ $\mu\text{s}$
Settling Time	$t_s$	To 0.01%, $V_{IN} = 10\text{ V step}$ , $R_L = 1\text{ k}\Omega$		3		$\mu\text{s}$
Gain Bandwidth Product	GBP	$R_L = 1\text{ M}\Omega$ , $C_L = 35\text{ pF}$ , $A_V = 1$		6.5		MHz
Phase Margin	$\Phi_M$	$R_L = 1\text{ M}\Omega$ , $C_L = 35\text{ pF}$ , $A_V = 1$		60		Degrees
<b>THD + NOISE</b>						
Total Harmonic Distortion and Noise	THD + N	$R_L = 2\text{ k}\Omega$ , $A_V = 1$ , $V_{IN} = 3\text{ V rms}$ , $f = 1\text{ kHz}$		0.0002		%
<b>NOISE PERFORMANCE</b>						
Voltage Noise	$e_n$ p-p	$f = 0.1\text{ Hz to }10\text{ Hz}$		60		nV p-p
Voltage Noise Density	$e_n$	$f = 1\text{ kHz}$		2.8		nV/ $\sqrt{\text{Hz}}$
Current Noise Density	$i_n$	$f = 1\text{ kHz}$		1.2		pA/ $\sqrt{\text{Hz}}$

$V_{SY} = \pm 15\text{ V}$ ,  $V_{CM} = 0\text{ V}$ ,  $T_A = 25^\circ\text{C}$ , LFCSP package, unless otherwise noted.

Table 3.

Parameter	Symbol	Conditions	Min	Typ	Max	Unit
<b>INPUT CHARACTERISTICS</b>						
Offset Voltage	$V_{OS}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		0.3	1	mV
Input Bias Current	$I_B$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		30	100	nA
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			150	nA
Input Offset Current	$I_{OS}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		5	50	nA
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			75	nA
Input Voltage Range		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	-12.5		+12.5	V
Common-Mode Rejection Ratio	CMRR	$V_{CM} = -12.5\text{ V to }+12.5\text{ V}$	110	116		dB
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	106			dB
Large Signal Voltage Gain	$A_{VO}$	$R_L = 2\text{ k}\Omega$ , $V_O = -11\text{ V to }+11\text{ V}$	110	117		dB
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	102			dB
		$R_L = 600\ \Omega$ , $V_O = -10\text{ V to }+10\text{ V}$	108	117		dB
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	100			dB
Offset Voltage Drift	$\Delta V_{OS}/\Delta T$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		3		$\mu\text{V}/^\circ\text{C}$
Input Resistance, Differential Mode	$R_{INDM}$			1.5		M $\Omega$
Input Resistance, Common Mode	$R_{INCM}$			500		M $\Omega$
Input Capacitance, Differential Mode	$C_{INDM}$			2.4		pF
Input Capacitance, Common Mode	$C_{INCM}$			2.1		pF
<b>OUTPUT CHARACTERISTICS</b>						
Output Voltage High	$V_{OH}$	$R_L = 2\text{ k}\Omega$ to GND	12.8	13		V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12.5			V
		$R_L = 600\ \Omega$ to GND	12.4	12.8		V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	12			V
		$V_{SY} = \pm 18\text{ V}$ , $R_L = 600\ \Omega$ to GND	15	15.8		V
Output Voltage Low	$V_{OL}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	14			V
		$R_L = 2\text{ k}\Omega$ to GND		-14	-13.6	V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			-13	V
		$R_L = 600\ \Omega$ to GND		-13.6	-13	V
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			-12.5	V
		$V_{SY} = \pm 18\text{ V}$ , $R_L = 600\ \Omega$ to GND		-16.6	-16	V
Short-Circuit Current	$I_{SC}$	$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		40		mA
					-15	V
Closed-Loop Output Impedance	$Z_{OUT}$	$f = 1\text{ kHz}$ , $A_V = 1$		0.1		$\Omega$
<b>POWER SUPPLY</b>						
Power Supply Rejection Ratio	PSRR	$V_{SY} = \pm 4.5\text{ V to } \pm 18\text{ V}$	100	104		dB
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$	95			dB
Supply Current per Amplifier	$I_{SY}$	$V_{SY} = \pm 4.5\text{ V to } \pm 18\text{ V}$ , $I_O = 0\text{ mA}$		1.8	2.25	mA
		$-40^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$			3.35	mA
<b>DYNAMIC PERFORMANCE</b>						
Slew Rate	SR	$R_L = 2\text{ k}\Omega$ , $A_V = 1$		12		V/ $\mu\text{s}$
Settling Time	$t_s$	To 0.01%, $V_{IN} = 10\text{ V step}$ , $R_L = 1\text{ k}\Omega$		3		$\mu\text{s}$
Gain Bandwidth Product	GBP	$R_L = 1\text{ M}\Omega$ , $C_L = 35\text{ pF}$ , $A_V = 1$		6.5		MHz
Phase Margin	$\Phi_M$	$R_L = 1\text{ M}\Omega$ , $C_L = 35\text{ pF}$ , $A_V = 1$		60		Degrees
<b>THD + NOISE</b>						
Total Harmonic Distortion and Noise	THD + N	$R_L = 2\text{ k}\Omega$ , $A_V = 1$ , $V_{IN} = 3\text{ V rms}$ , $f = 1\text{ kHz}$		0.0002		%
<b>NOISE PERFORMANCE</b>						
Voltage Noise	$e_n$ p-p	$f = 0.1\text{ Hz to }10\text{ Hz}$		60		nV p-p
Voltage Noise Density	$e_n$	$f = 1\text{ kHz}$		2.8		nV/ $\sqrt{\text{Hz}}$
Current Noise Density	$i_n$	$f = 1\text{ kHz}$		1.2		pA/ $\sqrt{\text{Hz}}$

## ABSOLUTE MAXIMUM RATINGS

Table 4.

Parameter	Rating
Supply Voltage	±20 V
Input Voltage	±V <sub>SY</sub>
Input Current <sup>1</sup>	±10 mA
Differential Input Voltage	±1.2 V
Output Short-Circuit Duration to GND	Indefinite
Storage Temperature Range	−65°C to +150°C
Operating Temperature Range	−40°C to +125°C
Junction Temperature Range	−65°C to +150°C
Lead Temperature (Soldering, 60 sec)	300°C

<sup>1</sup>The input pins have clamp diodes to the power supply pins.

Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. This is a stress rating only; functional operation of the device at these or any other conditions above those indicated in the operational section of this specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

## THERMAL RESISTANCE

$\theta_{JA}$  is specified for the worst-case conditions, that is, a device soldered in a circuit board for surface-mount packages. This was measured using a standard 4-layer board.

Table 5. Thermal Resistance

Package Type	$\theta_{JA}$	$\theta_{JC}$	Unit
8-Lead SOIC	158	43	°C/W
8-Lead LFCSP	115	40	°C/W

## POWER SEQUENCING

The op amp supplies must be established simultaneously with, or before, any input signals that are applied. If this is not possible, limit the input current to 10 mA.

## ESD CAUTION



**ESD (electrostatic discharge) sensitive device.** Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.

# TYPICAL PERFORMANCE CHARACTERISTICS

T<sub>A</sub> = 25°C, unless otherwise noted.

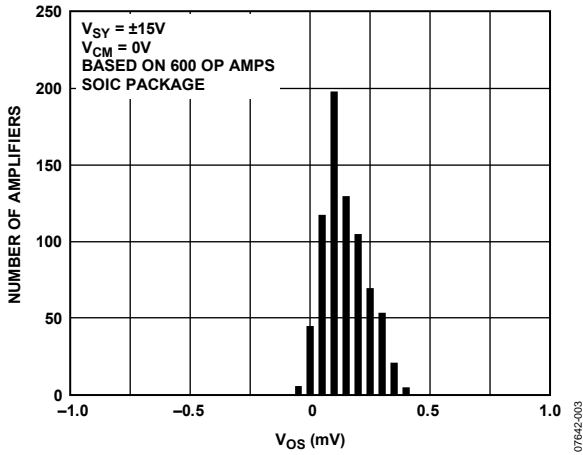


Figure 3. Input Offset Voltage Distribution

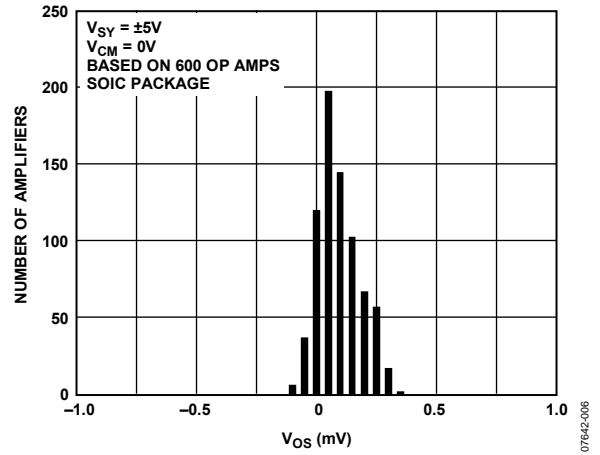


Figure 6. Input Offset Voltage Distribution

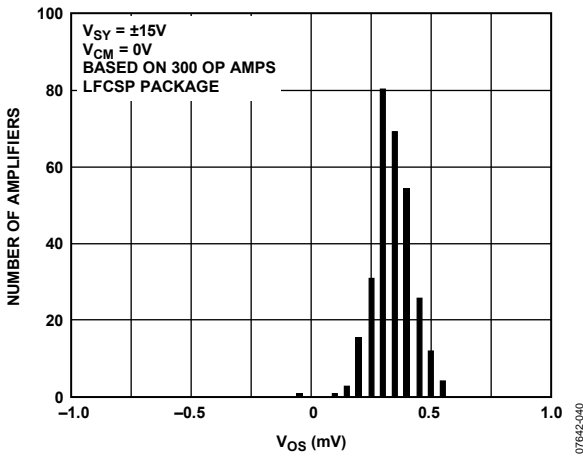


Figure 4. Input Offset Voltage Distribution

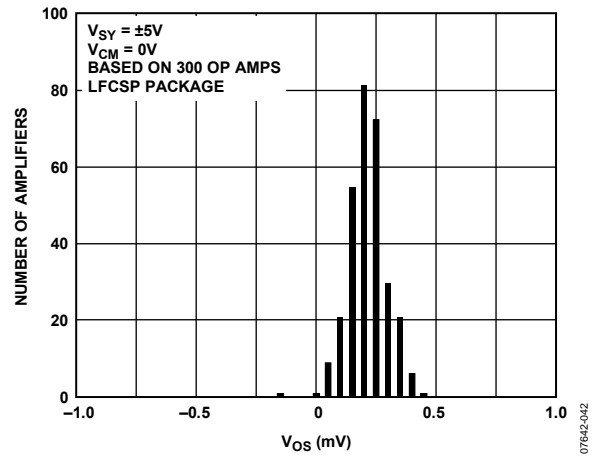


Figure 7. Input Offset Voltage Distribution

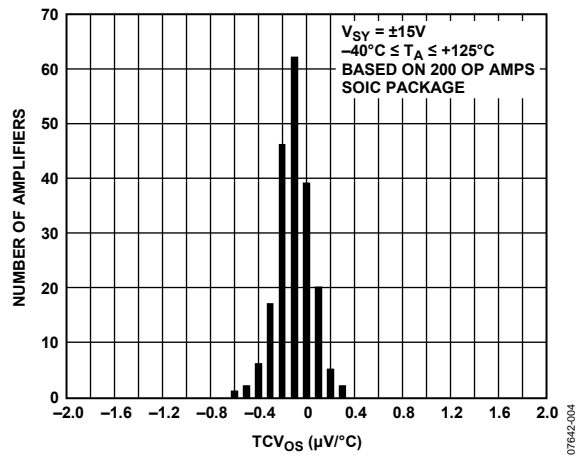


Figure 5. Input Offset Voltage Drift Distribution

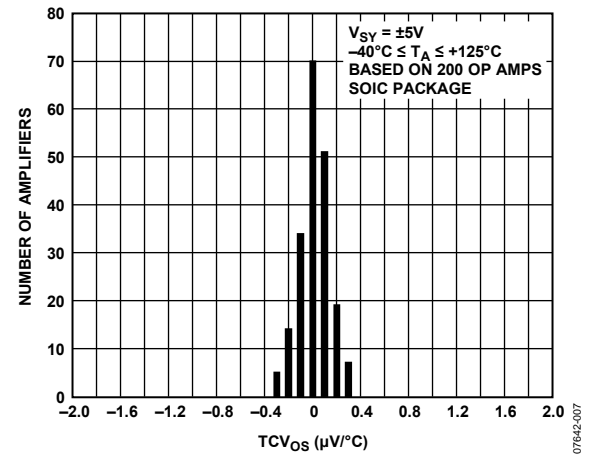


Figure 8. Input Offset Voltage Drift Distribution

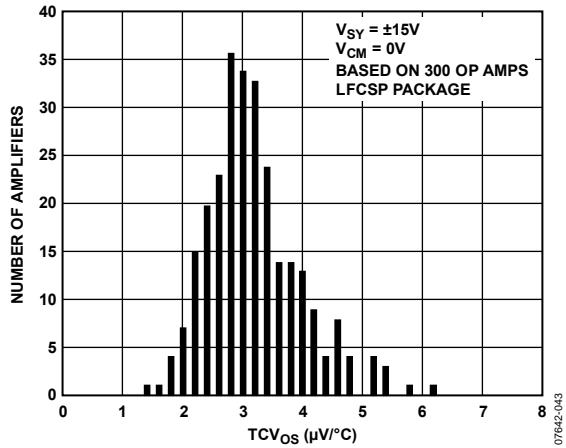


Figure 9. Input Offset Voltage Drift Distribution

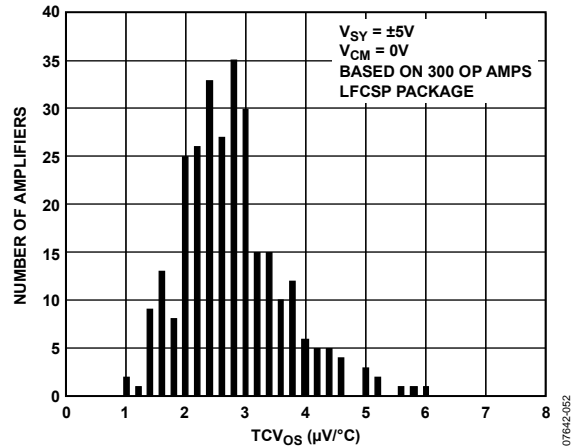


Figure 12. Input Offset Voltage Drift Distribution

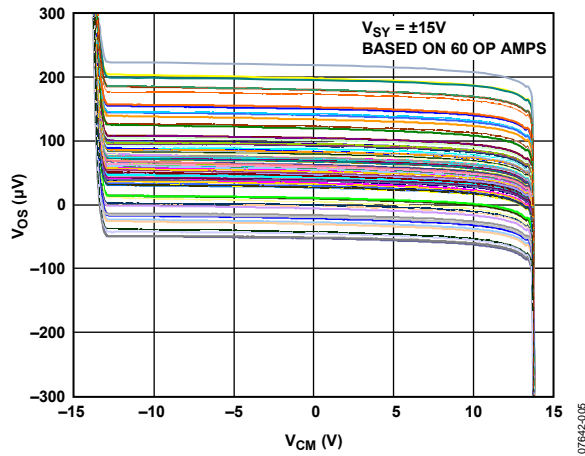


Figure 10. Input Offset Voltage vs. Common-Mode Voltage

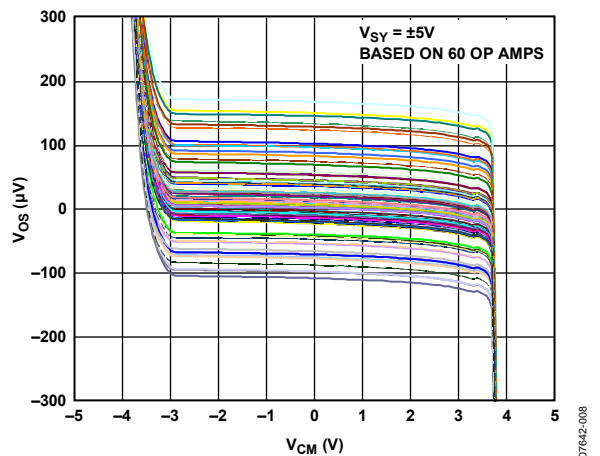


Figure 13. Input Offset Voltage vs. Common-Mode Voltage

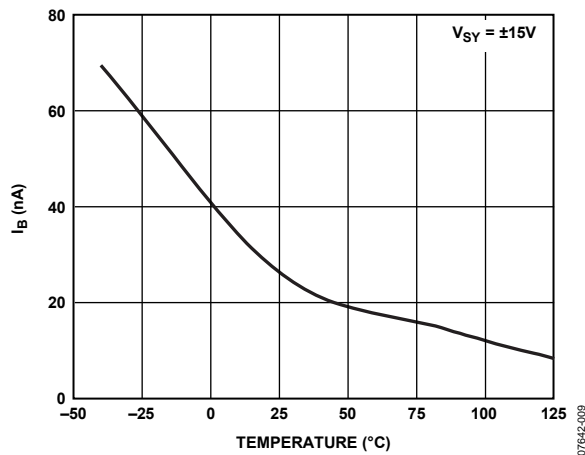


Figure 11. Input Bias Current vs. Temperature

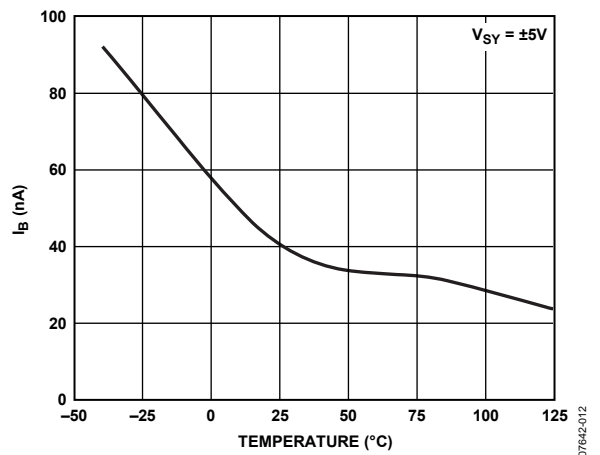


Figure 14. Input Bias Current vs. Temperature

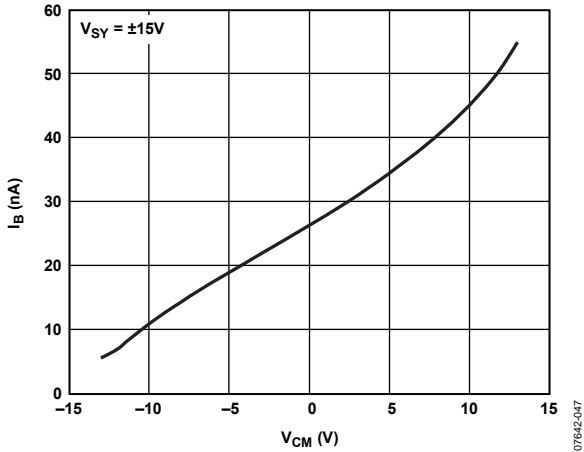


Figure 15. Input Bias Current vs. Input Common-Mode Voltage

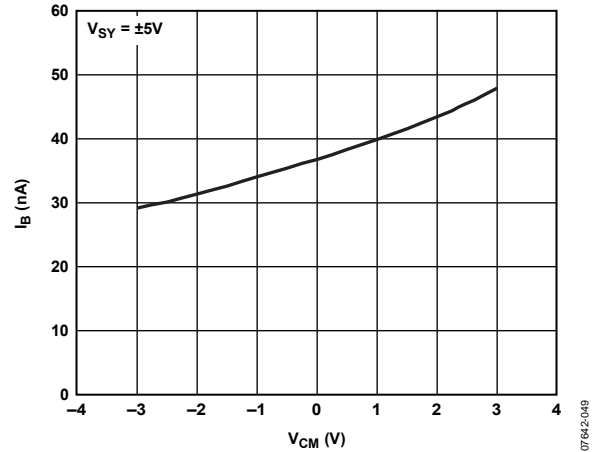


Figure 18. Input Bias Current vs. Input Common-Mode Voltage

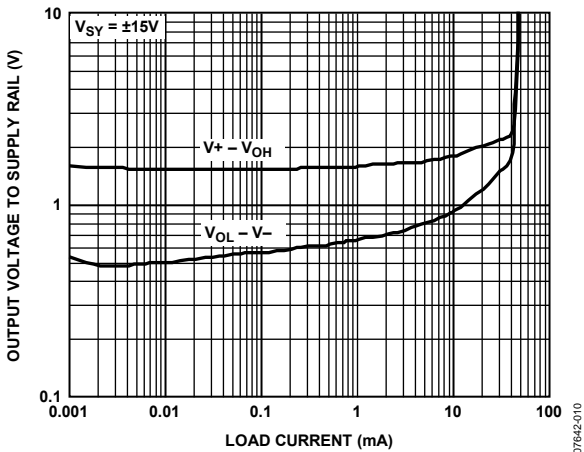


Figure 16. Output Voltage to Supply Rail vs. Load Current

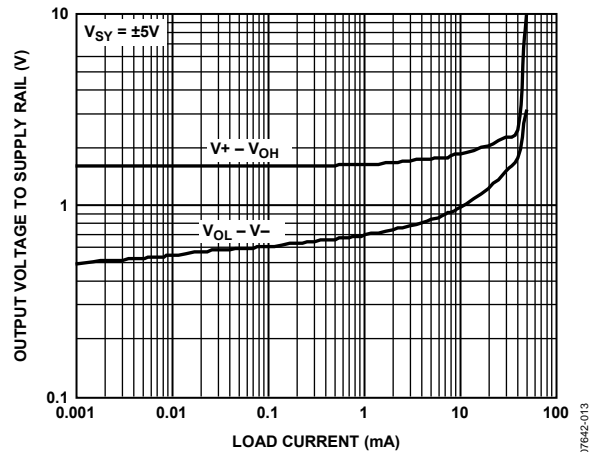


Figure 19. Output Voltage to Supply Rail vs. Load Current

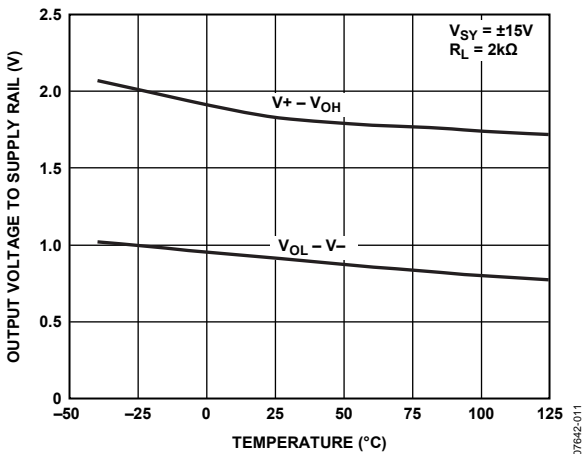


Figure 17. Output Voltage to Supply Rail vs. Temperature

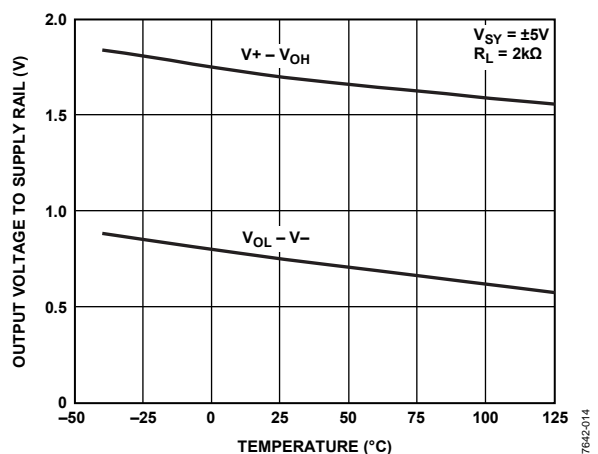


Figure 20. Output Voltage to Supply Rail vs. Temperature



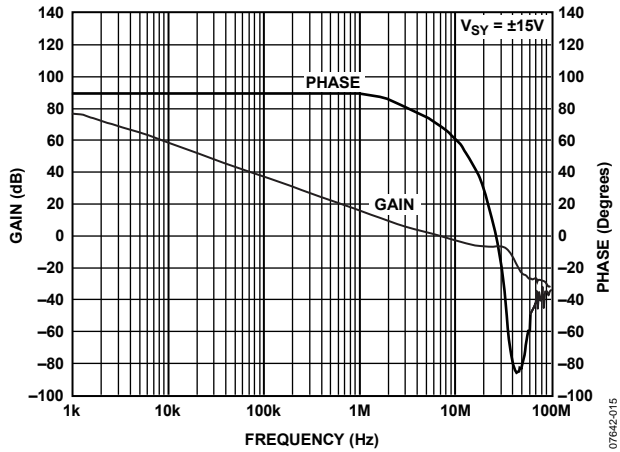


Figure 21. Open-Loop Gain and Phase vs. Frequency

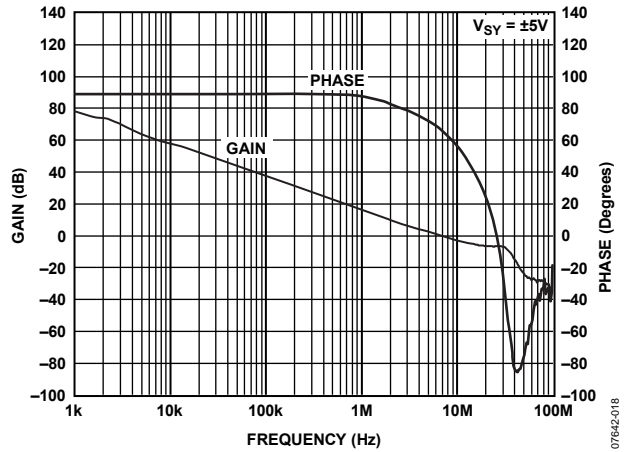


Figure 24. Open-Loop Gain and Phase vs. Frequency

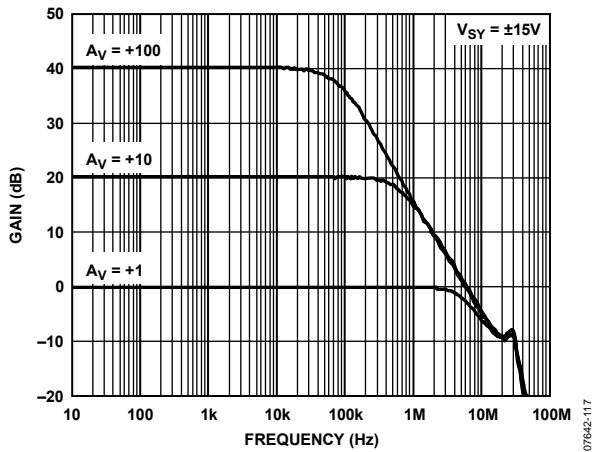


Figure 22. Closed-Loop Gain vs. Frequency

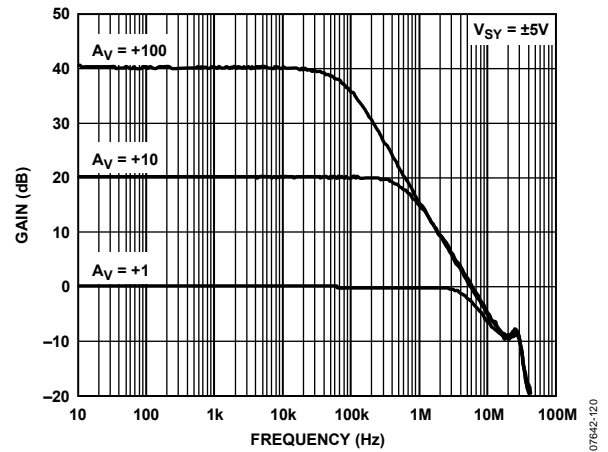


Figure 25. Closed-Loop Gain vs. Frequency

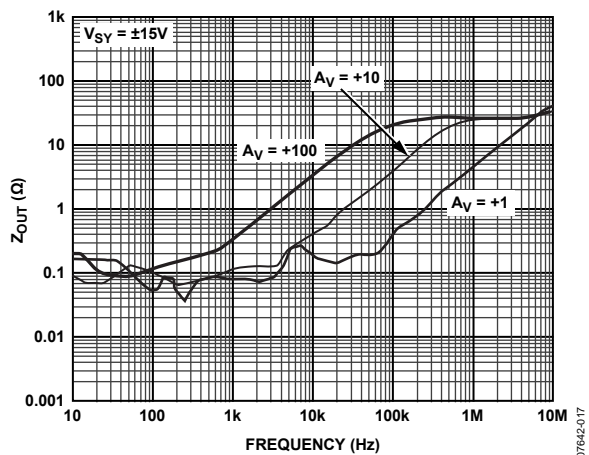


Figure 23. Output Impedance vs. Frequency

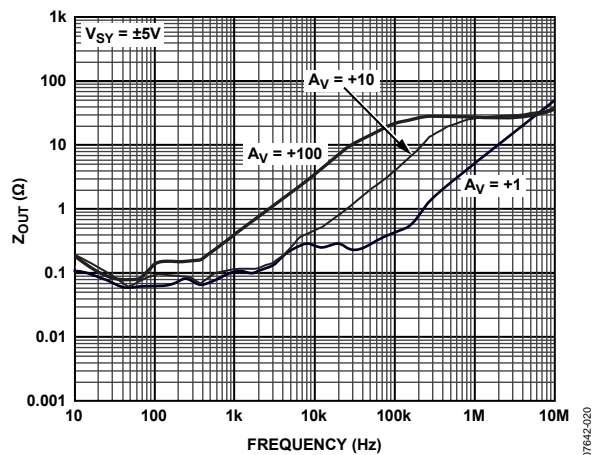


Figure 26. Output Impedance vs. Frequency

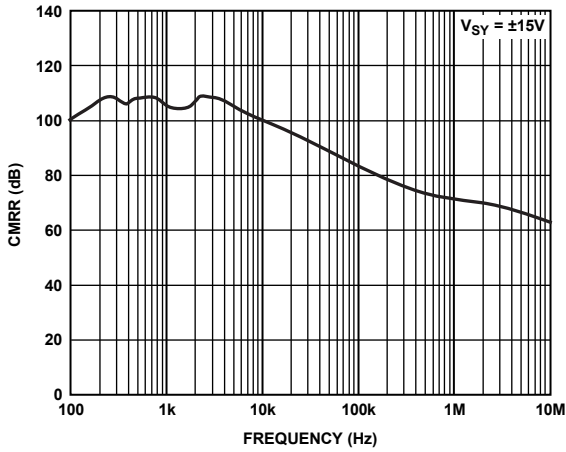


Figure 27. CMRR vs. Frequency

07642-021

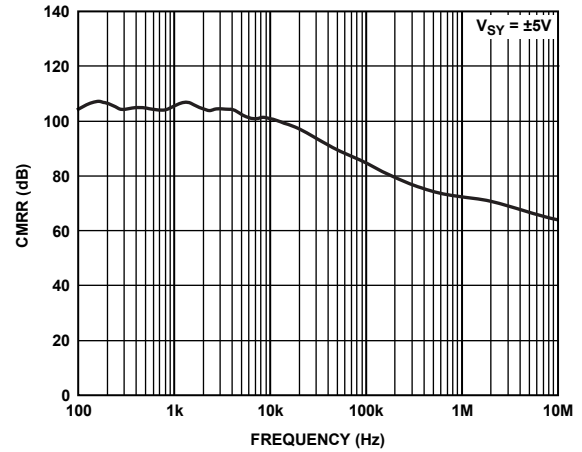


Figure 30. CMRR vs. Frequency

07642-024

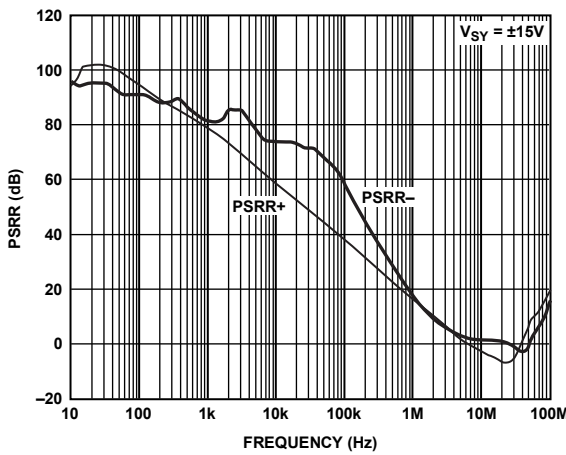


Figure 28. PSRR vs. Frequency

07642-022

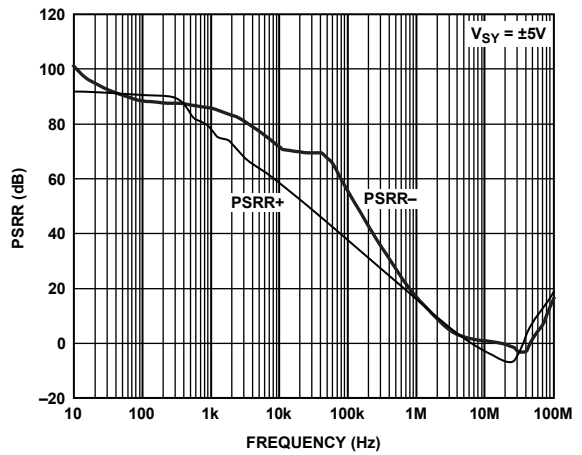


Figure 31. PSRR vs. Frequency

07642-025

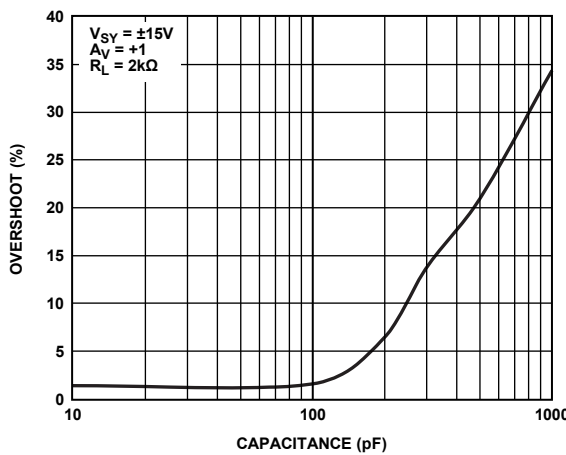


Figure 29. Small Signal Overshoot vs. Load Capacitance

07642-023

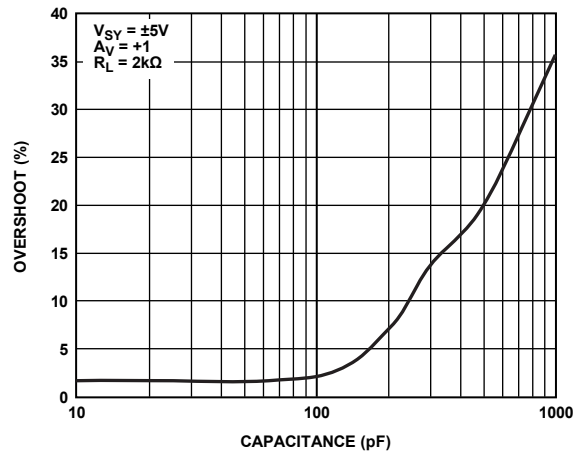


Figure 32. Small Signal Overshoot vs. Load Capacitance

07642-026

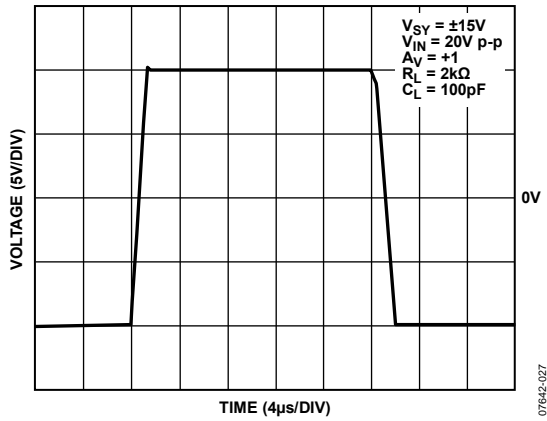


Figure 33. Large Signal Transient Response

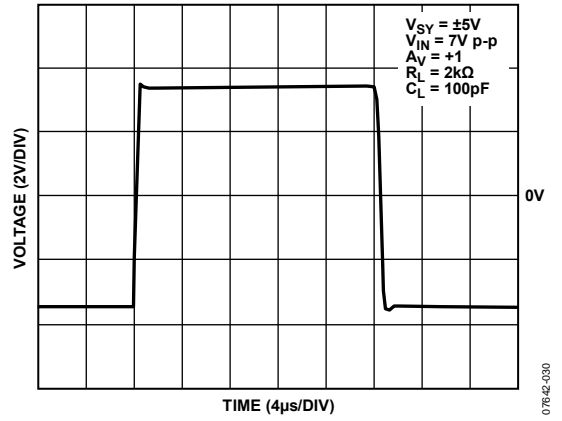


Figure 36. Large Signal Transient Response

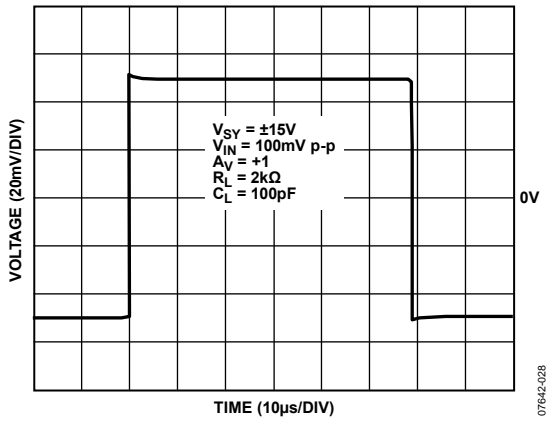


Figure 34. Small Signal Transient Response

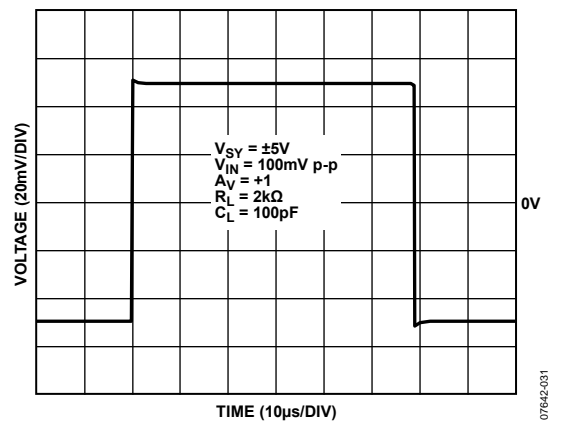


Figure 37. Small Signal Transient Response

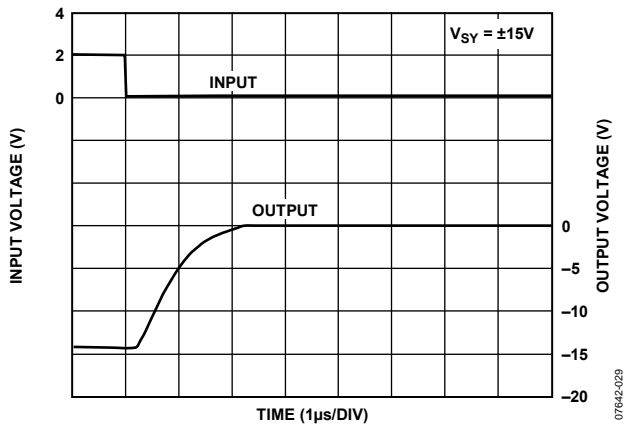


Figure 35. Negative Overload Recovery

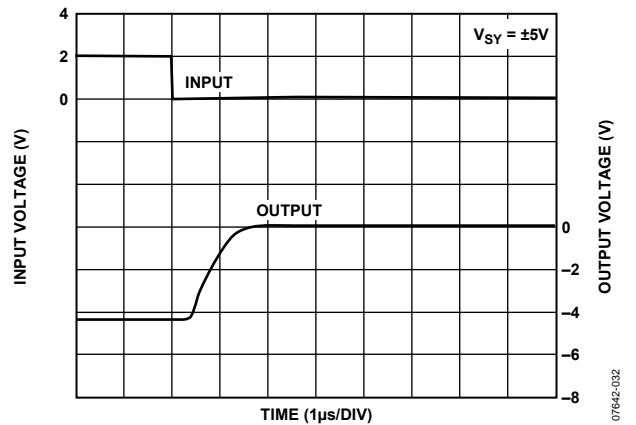


Figure 38. Negative Overload Recovery

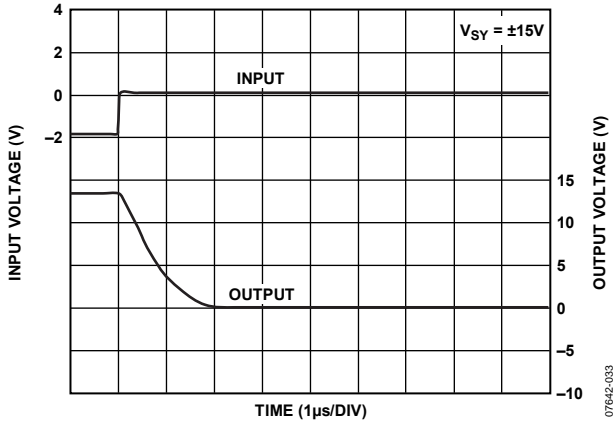


Figure 39. Positive Overload Recovery

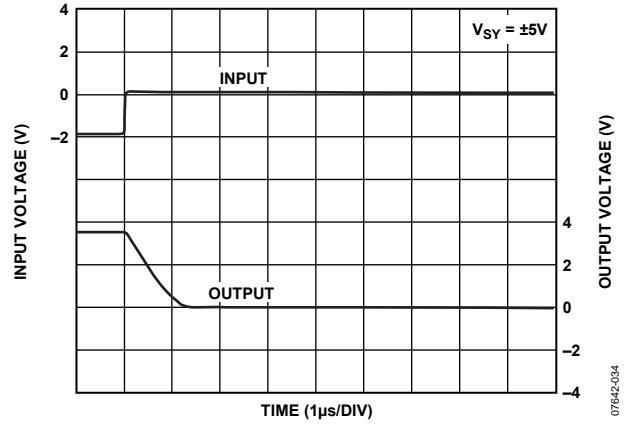


Figure 42. Positive Overload Recovery

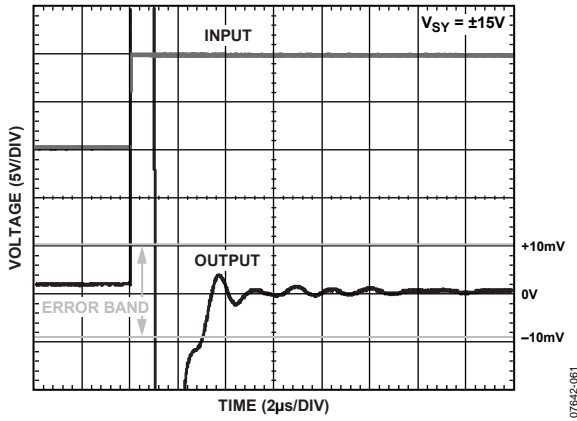


Figure 40. Positive Settling Time to 0.01%

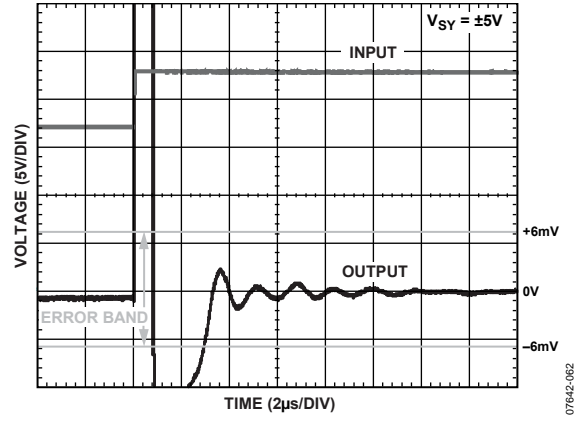


Figure 43. Positive Settling Time to 0.01%

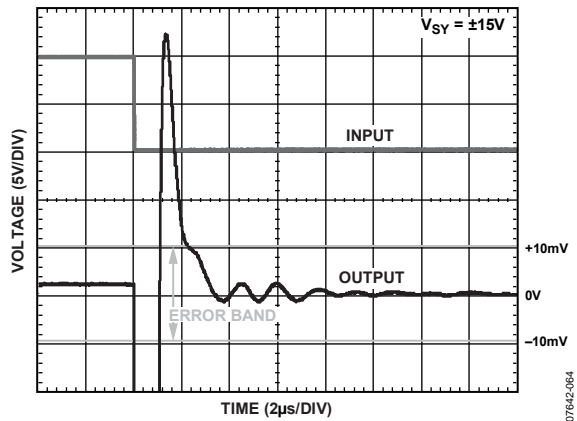


Figure 41. Negative Settling Time to 0.01%

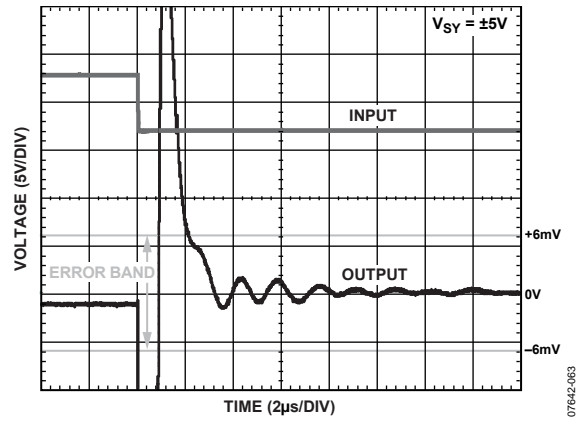


Figure 44. Negative Settling Time to 0.01%

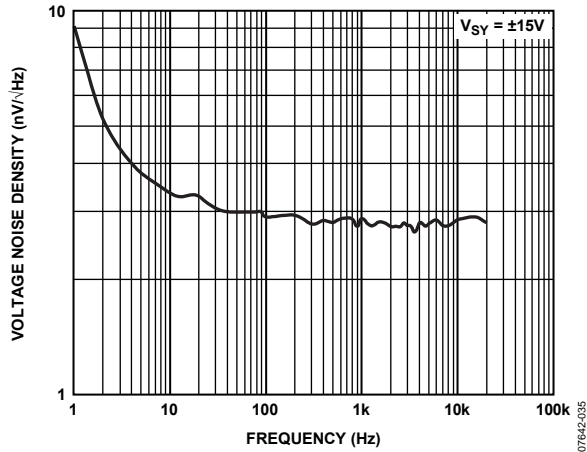


Figure 45. Voltage Noise Density

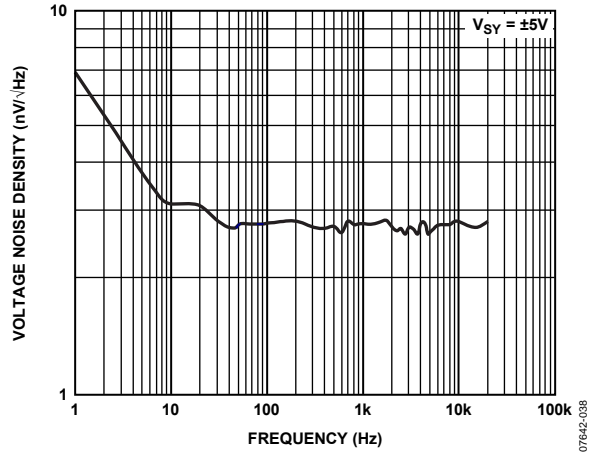


Figure 48. Voltage Noise Density

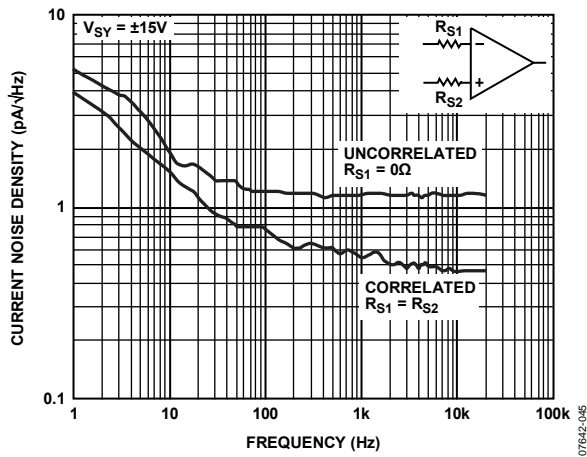


Figure 46. Current Noise Density

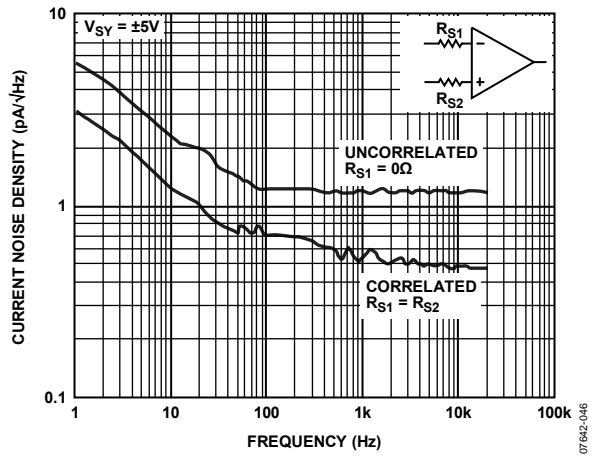


Figure 49. Current Noise Density

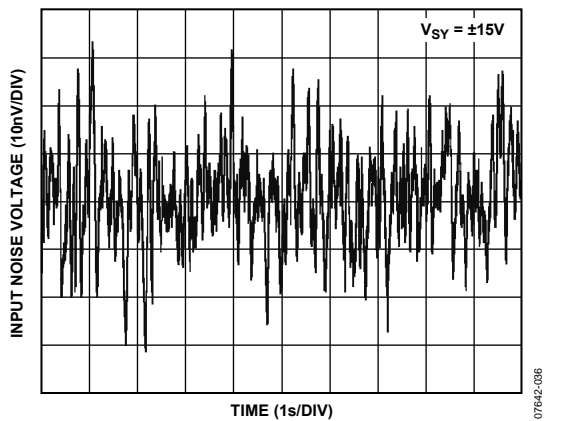


Figure 47. 0.1 Hz to 10 Hz Noise

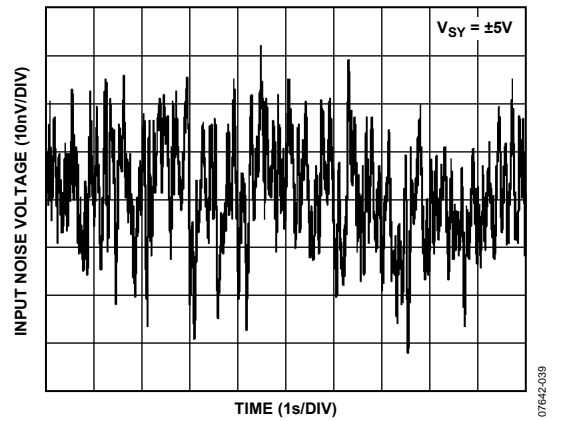


Figure 50. 0.1 Hz to 10 Hz Noise

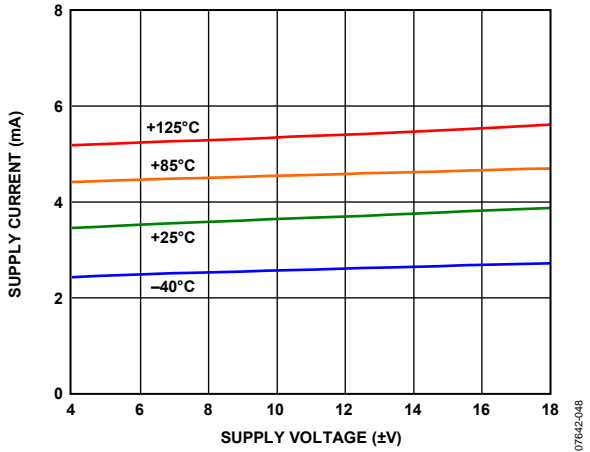


Figure 51. Supply Current vs. Supply Voltage

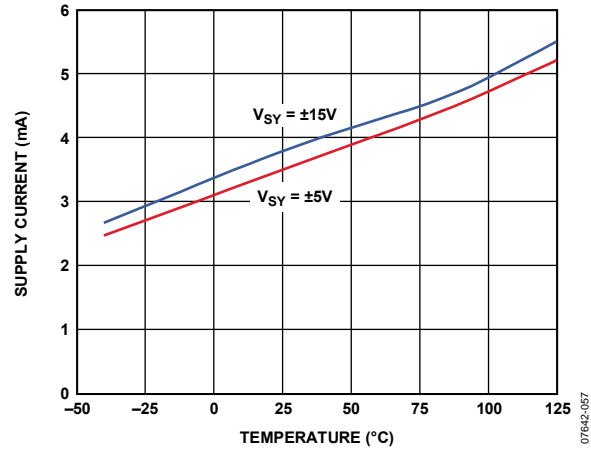


Figure 54. Supply Current vs. Temperature

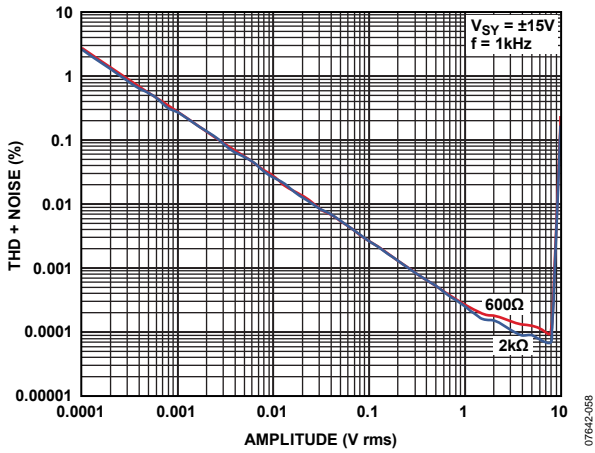


Figure 52. THD + Noise vs. Amplitude

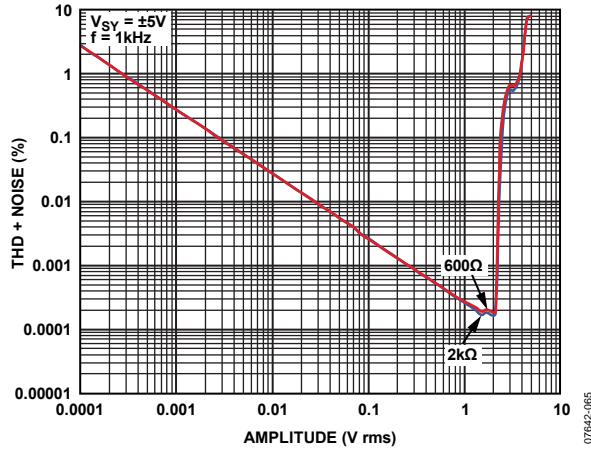


Figure 55. THD + Noise vs. Amplitude

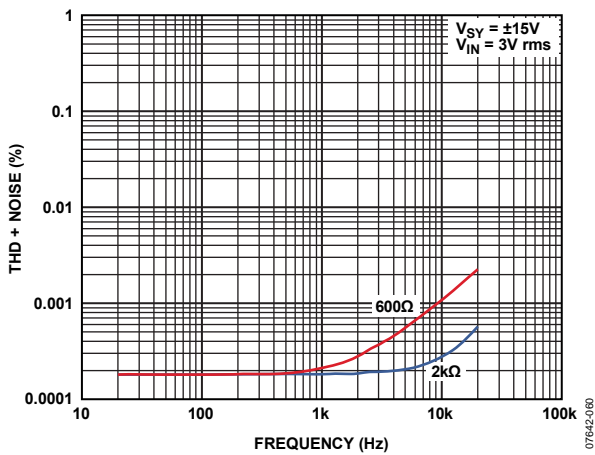


Figure 53. THD + Noise vs. Frequency

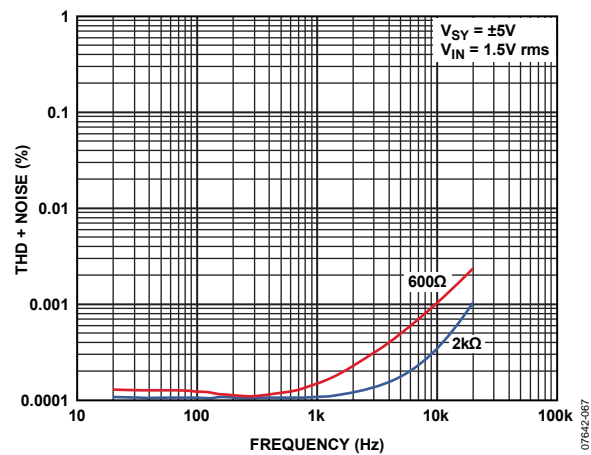


Figure 56. THD + Noise vs. Frequency

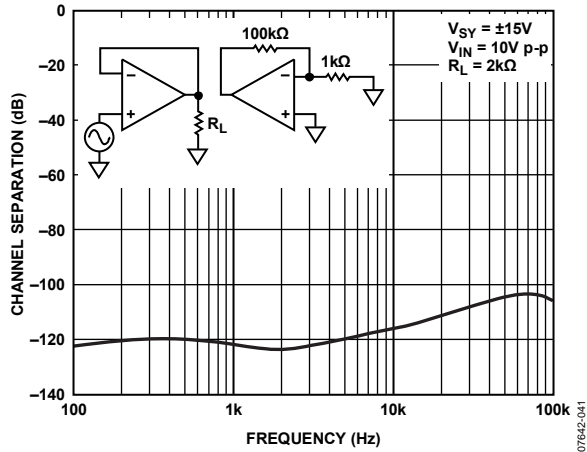


Figure 57. Channel Separation vs. Frequency

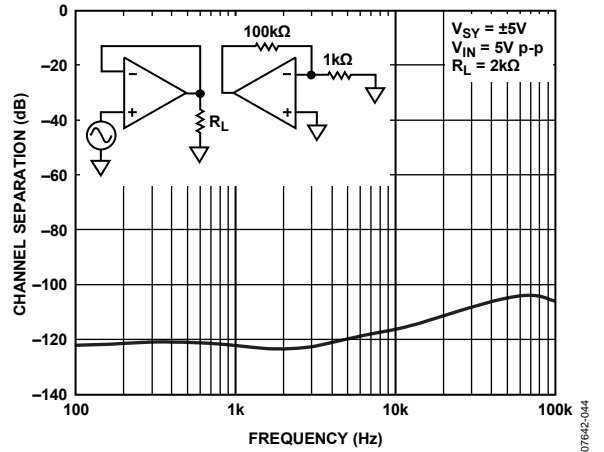


Figure 60. Channel Separation vs. Frequency

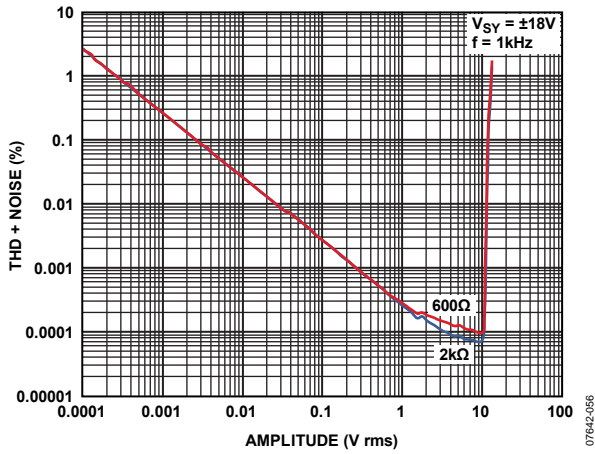


Figure 58. THD + Noise vs. Amplitude

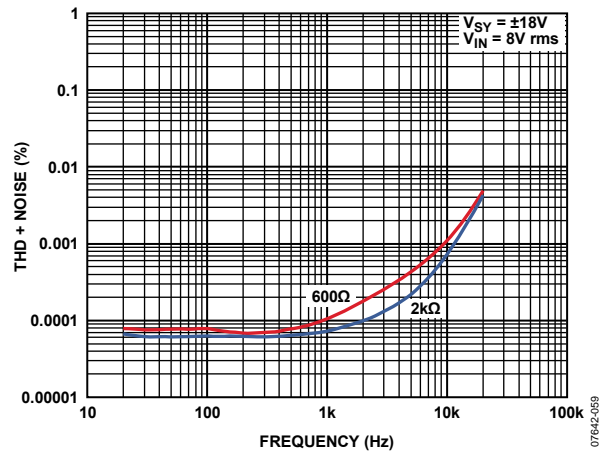


Figure 61. THD + Noise vs. Frequency

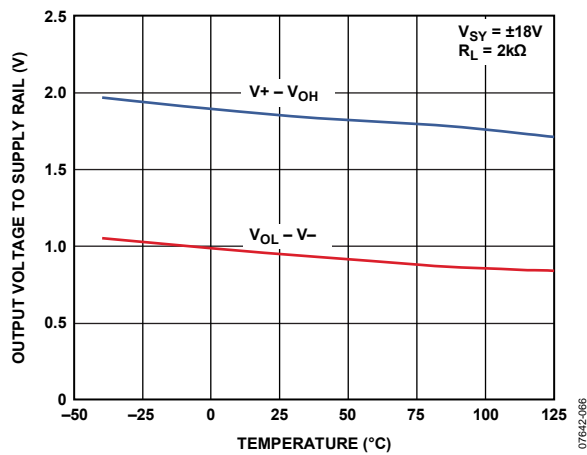


Figure 59. Output Voltage to Supply Rail vs. Temperature

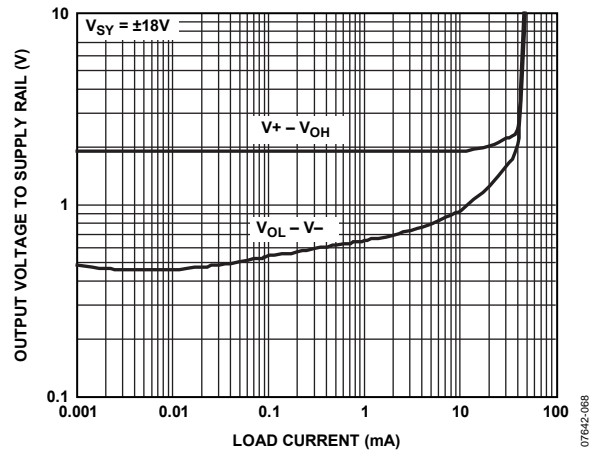


Figure 62. Output Voltage to Supply Rail vs. Load Current

## APPLICATIONS INFORMATION

### INPUT PROTECTION

To prevent base-emitter junction breakdown from occurring in the input stage of the ADA4075-2 when a very large differential voltage is applied, the inputs are clamped by the internal diodes to  $\pm 1.2$  V. To preserve the ultralow voltage noise feature of the ADA4075-2, the commonly used internal current-limiting resistors in series with the inputs are not used.

In small signal applications, current limiting is not required; however, in applications where the differential voltage of the ADA4075-2 exceeds  $\pm 1.2$  V, large currents may flow through these diodes. Employ external current-limiting resistors as shown in Figure 63 to reduce the input currents to less than  $\pm 10$  mA. Note that depending on the value of these resistors, the total voltage noise will most likely be degraded. For example, a 1 k $\Omega$  resistor at room temperature has a thermal noise of 4 nV/ $\sqrt{\text{Hz}}$ , whereas the ADA4075-2 has an ultralow voltage noise of only 2.8 nV/ $\sqrt{\text{Hz}}$  typical.

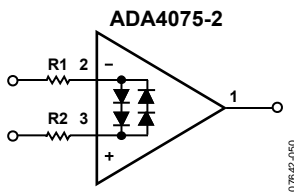


Figure 63. Input Protection

### TOTAL HARMONIC DISTORTION

The total harmonic distortion + noise (THD + N) of the ADA4075-2 is 0.0002% typical with a load resistance of 2 k $\Omega$ . Figure 64 shows the performance of the ADA4075-2 driving a 2 k $\Omega$  load with supply voltages of  $\pm 4$  V and  $\pm 15$  V. Notice that there is more distortion for the supply voltage of  $\pm 4$  V than for a supply voltage of  $\pm 15$  V. Therefore, it is important to operate the ADA4075-2 at a supply voltage greater than  $\pm 5$  V for optimum distortion. The THD + noise graphs for supply voltages of  $\pm 5$  V and  $\pm 18$  V are available in Figure 56 and Figure 61.

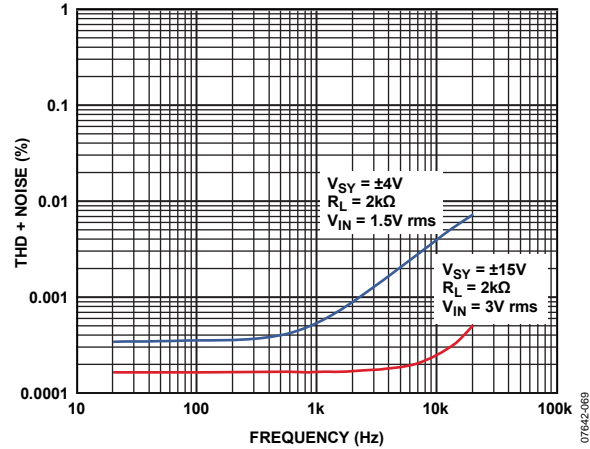


Figure 64. THD + Noise vs. Frequency

### PHASE REVERSAL

An undesired phenomenon, phase reversal (also known as phase inversion) occurs in many op amps when one or both of the inputs are driven beyond the specified input common-mode voltage ( $V_{ICM}$ ) range, in effect reversing the polarity of the output. In some cases, phase reversal can induce lockups and cause equipment damage as well as self destruction.

The ADA4075-2 incorporates phase reversal prevention circuitry that clamps the output to 2 V typical from the supply rails when one or both inputs exceed the  $V_{ICM}$  range. Figure 65 shows the input/output waveforms of the ADA4075-2 configured as a unity-gain buffer for a supply voltage of  $\pm 15$  V.

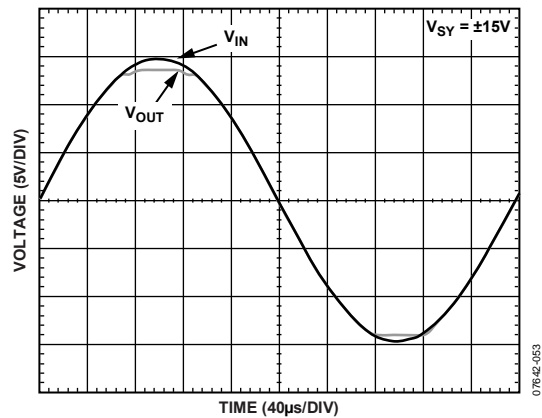


Figure 65. No Phase Reversal



**DAC OUTPUT FILTER**

The ultralow voltage noise, low distortion, and high slew rate of the ADA4075-2 make it an ideal choice for professional audio signal processing. Figure 66 shows the ADA4075-2 used in a typical audio DAC output filter configuration. The differential outputs of the DAC are fed into the ADA4075-2. The ADA4075-2 is configured as a differential Sallen-Key filter. It operates as an external low-pass filter to remove high frequency noise present on the output pins of the DAC. It also provides differential-to-single-ended conversion from the differential outputs of the DAC.

For a DAC output filter, an op amp with reasonable slew rate and bandwidth is required. The ADA4075-2 has a high slew rate of the 12 V/ $\mu$ s and a relatively wide bandwidth of 6.5 MHz. The cutoff frequency of the low-pass filter is approximately 167 kHz. In addition, the 100 k $\Omega$  – 47  $\mu$ F RC network provides ac coupling to block out the dc components at the output.

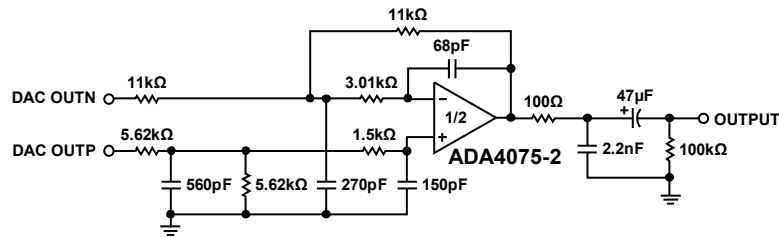


Figure 66. Typical DAC Output Filter Circuit (Differential)

07642-164

**BALANCED LINE DRIVER**

The circuit of Figure 67 shows a balanced line driver designed for audio use. Such drivers are intended to mimic an output transformer in operation, whereby the common-mode voltage can be impressed by the load. Furthermore, either output can be shorted to ground in single-ended applications without affecting the overall operation.

Circuits of this type use positive and negative feedback to obtain a high common-mode output impedance, and they are somewhat notorious for component sensitivity and susceptibility to latch-up. This circuit uses several techniques to avoid spurious behavior.

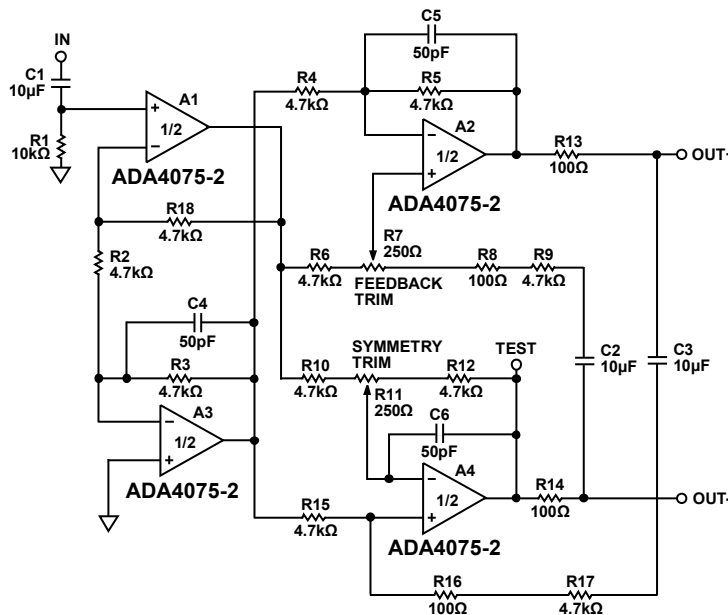
First, the 4-op-amp arrangement ensures that the input impedance is load independent (the input impedance can become negative with some configurations). Note that the output op amps are packaged with the input op amps to maximize drive capability.

Second, the positive feedback is ac-coupled by C2 and C3, which eliminates the need for offset trim. Because the circuit is ac-coupled at the input, these capacitors do not have significant dc voltage across them, thus tantalum types of capacitors can be used.

Finally, even with these precautions, it is vital that the positive feedback be accurately controlled. This is partly achieved by using 1% resistors. In addition, the following setup procedure ensures that the positive feedback does not become excessive:

1. Set R11 to its midposition (or short the ends together, whichever is easier) and temporarily short the negative output to ground.
2. Apply a 10 V p-p sine wave at approximately 1 kHz to the input and adjust R7 to provide 930 mV p-p at TEST (see Figure 67).
3. Remove the short from the negative output (and across R11, if used) and adjust R11 until the output waveforms are symmetric.

The overall gain of the driver is equal to 2, which provides an extra 6 dB of headroom in balanced differential mode. The output noise is about -109 dBV in a 20 kHz bandwidth.



- NOTES  
 1. ALL RESISTORS SHOULD HAVE 1% TOLERANCE.  
 2. A1/A2 IN SAME PACKAGE; A3/A4 IN SAME PACKAGE.

Figure 67. Balanced Line Driver

0764c-073

### BALANCED LINE RECEIVER

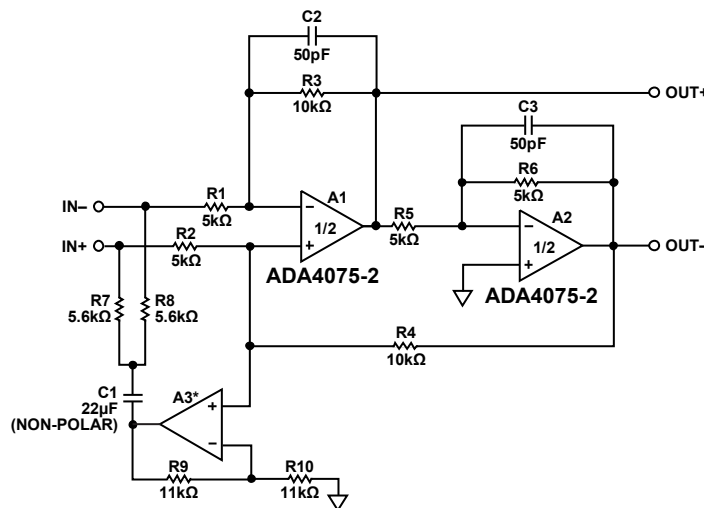
Figure 68 depicts a unity-gain balanced line receiver capable of a high degree of hum rejection. The CMRR is approximately given by

$$20 \log_{10} \left( \frac{R1 \times R4}{R2 \times R3} \right)$$

Therefore, R1 to R4 should be close tolerance components to obtain the best possible CMRR without adjustment. The presence of A2 ensures that the impedances are symmetric at the two inputs (unlike many other designs), and, as a bonus, A2 also provides a complementary output. A3 raises the common-mode input impedance from approximately 7.5 kΩ to approximately 70 kΩ, reducing the degradation of CMRR due to mismatches in source impedance.

Note that A3 is not in the signal path, and almost any op amp works well here. Although it may seem as though the inverting output should be noisier than the noninverting one, they are in fact symmetric at about -111 dBV (20 kHz bandwidth).

Sometimes an overall gain of ½ is desired to provide an extra 6 dB of differential input headroom. This can be attained by reducing R3 and R4 to 5 kΩ and increasing R9 to 22 kΩ.



\*A3 REDUCES THE DEGRADATION OF CMRR  
(SEE THE BALANCED LINE RECEIVER SECTION FOR MORE DETAILS).

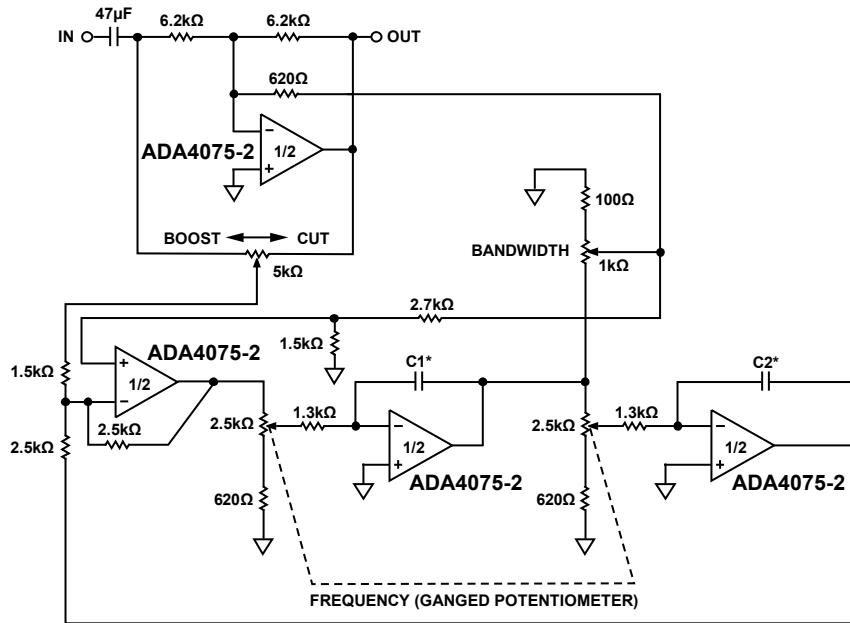
Figure 68. Balanced Line Receiver

07642-071

**LOW NOISE PARAMETRIC EQUALIZER**

The circuit in Figure 69 is a reciprocal parametric equalizer yielding  $\pm 20$  dB of cut or boost with variable bandwidth and frequency. The frequency control range is 6.9:1, with the geometric mean center frequency conveniently occurring at the midpoint of the potentiometer setting. The center frequency is equal to  $48 \text{ Hz}/C_t$ , where  $C_t$  is the value of  $C_1$  and  $C_2$  in microfarads.

The bandwidth control adjusts the Q from 0.9 to about 11. The overall noise is setting dependent, but with all controls centered, it is about  $-104 \text{ dBV}$  in a 20 kHz bandwidth. Such a low noise level can obviate the need for a bypass switch in many applications.



\*THE CENTER FREQUENCY IS AFFECTED BY THE VALUE OF  $C_1$  AND  $C_2$  (SEE THE LOW NOISE PARAMETRIC EQUALIZER SECTION FOR MORE DETAILS).

Figure 69. Low Noise Parametric Equalizer

07642-074

**SCHEMATIC**

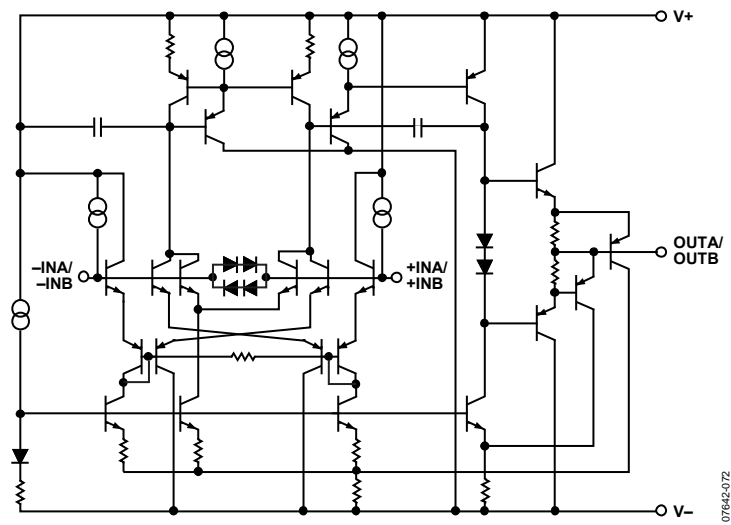
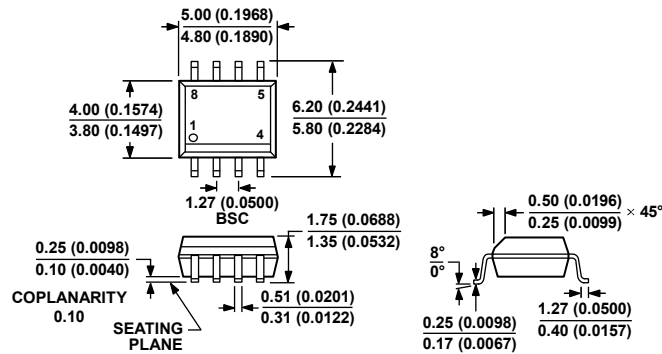


Figure 70. Simplified Schematic

07642-07Z

OUTLINE DIMENSIONS



COMPLIANT TO JEDEC STANDARDS MS-012-AA  
 CONTROLLING DIMENSIONS ARE IN MILLIMETERS; INCH DIMENSIONS  
 (IN PARENTHESES) ARE ROUNDED-OFF MILLIMETER EQUIVALENTS FOR  
 REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 71. 8-Lead Standard Small Outline Package [SOIC\_N]  
 Narrow Body (R-8)  
 Dimensions shown in millimeters and (inches)

012407-A

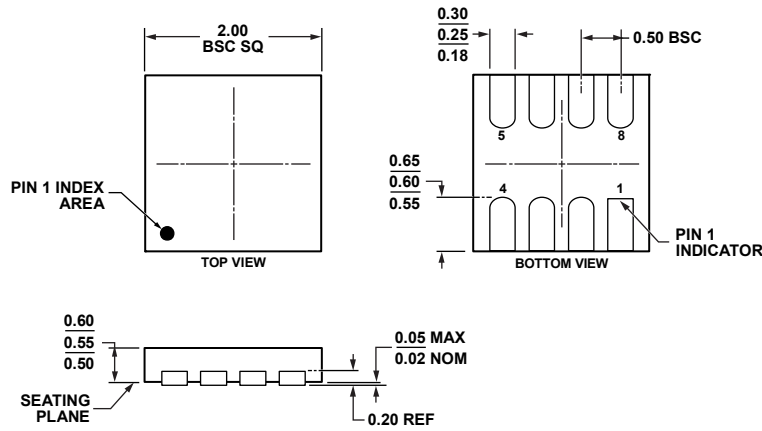


Figure 72. 8-Lead Lead Frame Chip Scale Package [LFCS\_P\_WD]  
 2 mm x 2 mm Body, Very Very Thin, Dual Lead  
 (CP-8-6)  
 Dimensions shown in millimeters

051608-A

ORDERING GUIDE

Model <sup>1</sup>	Temperature Range	Package Description	Package Option	Branding
ADA4075-2ARZ	-40°C to +125°C	8-Lead SOIC_N	R-8	
ADA4075-2ARZ-R7	-40°C to +125°C	8-Lead SOIC_N	R-8	
ADA4075-2ARZ-RL	-40°C to +125°C	8-Lead SOIC_N	R-8	
ADA4075-2ACPZ-R7	-40°C to +125°C	8-Lead LFCS_P_WD	CP-8-6	A0
ADA4075-2ACPZ-RL	-40°C to +125°C	8-Lead LFCS_P_WD	CP-8-6	A0

<sup>1</sup> Z = RoHS Compliant Part.

**NOTES**

**NOTES**



## Данный компонент на территории Российской Федерации

### Вы можете приобрести в компании MosChip.

Для оперативного оформления запроса Вам необходимо перейти по данной ссылке:

<http://moschip.ru/get-element>

Вы можете разместить у нас заказ для любого Вашего проекта, будь то серийное производство или разработка единичного прибора.

В нашем ассортименте представлены ведущие мировые производители активных и пассивных электронных компонентов.

Нашей специализацией является поставка электронной компонентной базы двойного назначения, продукции таких производителей как XILINX, Intel (ex.ALTERA), Vicor, Microchip, Texas Instruments, Analog Devices, Mini-Circuits, Amphenol, Glenair.

Сотрудничество с глобальными дистрибьюторами электронных компонентов, предоставляет возможность заказывать и получать с международных складов практически любой перечень компонентов в оптимальные для Вас сроки.

На всех этапах разработки и производства наши партнеры могут получить квалифицированную поддержку опытных инженеров.

Система менеджмента качества компании отвечает требованиям в соответствии с ГОСТ Р ИСО 9001, ГОСТ РВ 0015-002 и ЭС РД 009

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